CRPA operation. The array is composed of three identical antennas, and each antenna consists of the radiating patch and parasitic strips to achieve circular polarization. To improve the isolation, the shape of each antenna was transformed from the conventional rectangular shape to the arc shape to maximize the edge-to-edge distance, and the ground slot was inserted for further improvement. The proposed array was fabricated, and its antenna characteristics were measured in a full anechoic chamber. The array showed that the reflection coefficient is -10.8 dB, and the bore-sight gain is 1.1 dBic. The axial ratio bandwidth is 16 MHz with the minimum value of 1.9 dB, and the HPBW is greater than 100°. The mutual coupling strength was improved by 9.1 dB compared to the rectangular-shaped antenna array due to the increased edge-to-edge distance, and the null depth was improved by 3.5 dB in the azimuth direction. The results demonstrate that the proposed array is suitable to increase the null depth at low-elevation angles with improved isolation characteristics.

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A Frequency-Independent Method for Computing the Physical Optics-Based Electromagnetic Fields Scattered From a Hyperbolic Surface

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Abstract—In this communication, we propose a frequency-independent approach, the numerical steepest descent path (NSDP) method, for computing the physical optics scattered electromagnetic field on the quadratic hyperbolic surface. Due to the highly oscillatory nature of the physical optics integral, the proposed method relies on deforming the integration path of the integral into the NSDP on the complex plane. Numerical results for the PO-based EM fields from the hyperbolic surface illustrate that the proposed NSDP method is frequency independent in computational cost and error controllable in accuracy.

Index Terms—Critical-point contributions, hyperbolic surface, numerical steepest descent path (NSDP), physical optics.

I. INTRODUCTION

In electromagnetics (EM), when the product of the external wave number k and the size of the considered object L, i.e., kL ranges from tens to thousands, the analysis of the scattered EM field belongs to the high frequency problem. In this case, the classical physical optics (PO) current approximation [1] has been accepted as an efficient method to calculate the PO-based EM fields scattered from the electrically large scatterers. PO-based EM fields $\mathbf{E}^{(s)}(\mathbf{r})$ from the considered perfect electric conductor scatterers can be represented as three surface integrals [3] of the type

$$I(k,\mathbf{r}) = \int_{\partial\Omega_1} s(\mathbf{r},\mathbf{r}') e^{ikv(\mathbf{r},\mathbf{r}')} dS(\mathbf{r}').$$
(1)

They are called the surface PO integrals, and $\partial\Omega_1$ denotes the surface of the lit region of the considered object, as shown in Fig. 1. The PO integrand in (1) contains the slowly varying amplitude term $s(\mathbf{r}, \mathbf{r}')$, and the exponential of the phase function term $e^{ikv(\mathbf{r}')}$. Due to the highly oscillatory phase behavior of the PO integrand, it is quite challenging to calculate the PO integral with frequency-independent workload and error controllable accuracy.

For the calculation of the PO-based EM fields, direct PO solvers [4]–[5] make the computational cost dramatically increase with k. In

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Fig. 1. PO current on the perfect electric conductor scatterer.

this sense, efficient algorithms for calculating the PO-based EM fields, especially frequency-independent algorithms, are in great demand. The traditional high-frequency asymptotic (HFA) approach [6]–[10] can provide the calculation of the PO-based EM fields with frequency-independent workload. In [10], the authors treated the PO integrals from a curved surface with curvilinear edges and relatively general boundary conditions. The canonical integrals in the uniform geometrical theory of diffraction (UTD) were used in the evaluation of PO integrals. Furthermore, the authors developed the efficient algorithm to calculate the "transition functions" in canonical integrals [11] and [12].

Recently, the numerical steepest descent path (NSDP) approach [16]–[20] provides an efficient way to evaluate the highly oscillatory PO integral. The similarity of our work and the work in [17] is that the contour deformation technique via steepest descent paths on the complex plane is adopted to evaluate these PO integrals. However, there are three main differences between these two works. First, in [17], the Abel's summation method, the Lebesgue integral theory and poles extraction technique in complex analysis were adopted for the development of NSDPs from the hyperbolic phase term. In this work, we avoid the Abel's summation and the Lebesgue integral theory and obtain all NSDPS. Second, in [17], the phase function g(x,y) = xy is considered. In this work, the phase function g(x,y) = $x^2 \pm y^2$ is considered via affine transformation technique. Hence, the NSDPs obtained in this communication are different from those in [17]. Importantly, we provide the NSDPs. Third, high-frequency wave physics, such as the contributions from the stationary phase point (SPP), the boundary resonance points, and the vertex points, was captured by the proposed NSDP method. In [21], for the computation of scattering from rough surfaces with very large surface heights, an acceleration algorithm was successfully developed by the steepest descent path contour deformation for the Hankel function. In [22], the equivalence between the modified edge representation line and the PO surface integration was developed by the Stokes theorem and the asymptotic technique. Furthermore, a criterion on the acceleration of the PO surface integration with the SPP method was clearly given.

The contributions in this work are that the PO-based EM fields from the hyperbolic patches are considered. Then, the integrand of the PO integral takes the hyperbolic phase behavior, which is different from the work in [19]. In this case, all NSDPs are changed and reconstructed compared to the work in [19]. With the high-frequency wave physics viewpoint, the formulations of the SPP and the boundary resonance point are all changed. Furthermore, the coalescence of high-frequency critical points is considered. We have considered the



Fig. 2. (a) Electromagnetic wave impinges on the quadratic hyperbolic surface $\partial\Omega$, governed by equation z = f(x, y). (b) Projection of $\partial\Omega$ onto the x-y plane, $\partial\Omega_{xy}$.

PO-based EM fields from the parabolic and hyperbolic quadratic surfaces, and have further adopted the NSDP algorithm knowledge to calculate the scattered fields.

This communication is organized as follows. In Section II, the PO-based EM fields from the hyperbolic surface is discussed. In Section III, the surface PO integral is first transformed into several highly oscillatory line integrals. Then, we propose the NSDP method to treat these highly oscillatory line integrals. High-frequency critical-point contributions on the derived NSDPs are extensively studied in Section IV. In Section V, numerical experiments are shown to verify the efficiency of the proposed NSDP method. We make the conclusion in Section VI.

II. SURFACE PHYSICAL OPTICS INTEGRAL ON THE QUADRATIC HYPERBOLIC SURFACE

In this communication, the time harmonic dependence of $e^{-i\omega t}$ is adopted for the EM wave. We consider that the EM wave is impinging on the quadratic hyperbolic surfaces $\partial\Omega$, as demonstrated in Fig. 2(a). The hyperbolic surface is governed by the quadratic equation z = f(x, y), i.e., f(x, y) is a second-order polynomial in the xycartesian coordinate system. For the PEC with the electric conductivity $\sigma = \infty$, we denote the size of the considered hyperbolic surface as $L = \text{diam}(\partial\Omega)$, and the distance of the observation point **r** to the origin as $r = |\mathbf{r}|$.

In this work, we consider the far-zone of the scatterer with $r \gg 2L^2/\lambda$ and the PO approximation of the accurate electric equivalent current. λ is the wavelength. Then, for the incident plane wave, $\mathbf{E}^{(i)}(\mathbf{r}) = \mathbf{E}_0^{(i)} e^{ik\hat{\mathbf{r}}^{(i)}\cdot\mathbf{r}}$, the PO-based EM fields can be written in (1), with



Fig. 3. (a) Highly oscillatory PO type integrand, $f(x) = (5 - 3x - x^2)e^{ik(-x^2+(ax+b)^2)}$, with k = 500. (b) The integration domain is defined on $\mathbf{V_1V_2V_3V_4}$, $[L_1, L_2] \times [ax + b, 0]$ for integrand $e^{ik(-x^2+y^2)}$ with a = 0.25, b = -0.5.

$$\mathbf{s}(\mathbf{r},\mathbf{r}') = -\frac{ike^{ikr}}{2\pi r}\hat{\mathbf{r}} \times \hat{\mathbf{r}} \times \left(\hat{\mathbf{n}}(\mathbf{r}') \times \hat{\mathbf{r}}^{(i)} \times \mathbf{E}_{0}^{(i)}\right)$$
(2)

$$v(\mathbf{r}, \mathbf{r}') = \left(\hat{\mathbf{r}}^{(i)} - \hat{\mathbf{r}}\right) \cdot \mathbf{r}'.$$
(3)

In (2) and (3), $\hat{\mathbf{r}} = \mathbf{r}/r$ and $\hat{\mathbf{r}}^{(i)} = \hat{\mathbf{k}}^{(i)}$ are the unit vector of \mathbf{r} and the unit vector of $\mathbf{k}^{(i)}$, respectively. $\hat{\mathbf{n}}(\mathbf{r})$ is the outward unit normal vector from the hyperbolic surface. Equations (1)–(3) are the bistatic scattered electric field under the PO approximation. The vector function $\mathbf{s}(\mathbf{r}')$ in (2) is known as the vector amplitude function, and $v(\mathbf{r}')$ in (3) is the phase function. The integrand of the vector PO surface integral in (1) is highly oscillatory when k goes large. The highly oscillatory property of the PO integrand makes the computational effort grow up dramatically with the increasing k, as depicted in Fig. 3(a). Furthermore, for the quadratic surface, the PO integrand of the scattered field in (1) contains the quadratic phase function term v(x, y) [19]. With the asymptotic technique, the steepest descent path method could be adopted to evaluate the PO integral in an efficient way.

To simplify the PO surface integral in (1) to its canonical form, we follow the procedure in [19]. First, we proceed the projection process from the surface $\partial\Omega$ to $\partial\Omega_{xy}$ with polygonal boundary in the x'y' plane, as shown in Fig. 2(b). Next, we conduct the affine transformation as that given in [19], $\partial\Omega_{xy}$ is transformed to another polygonal domain D. In this manner, the PO integral from the hyperbolic surface can be simplified into the following two canonical forms

$$I = \int_{D} p(x', y') e^{\pm ik \left(-x'^2 + y'^2\right)} dy' dx'.$$
 (4)

The x' and y' variables in the above integrand correspond to the integration variables in the x'y' plane. The amplitude function p(x',y') takes the formulation

$$p(x',y') = \alpha_1 + \alpha_2 x' + \alpha_3 y' + \alpha_4 {x'}^2 + \alpha_5 {y'}^2 + \alpha_6 x' y'$$
 (5)

and α_j are complex numbers, j = 1, 2, ..., 6. Here, the domain D is a polygonal domain on the x'-y' plane. In detail, we first decompose the surface into several smaller triangular patches. Hence, the polygonal boundary is formed after the discretization procedure.

III. NSDP METHOD

We assume D as the trapezoidal domain in (4), as shown in Fig. 3(b). We denote the x-values of vertex points V_1 and V_2 as L_1 and L_2 , respectively. The governing line equation for edge V_3V_4 is y = ax + b, with a > 0. The slope "a" of the edge y = ax + b could also be a < 0. Then, after a projection of the 3-D surface to a

plane of (x, y), the PO surface integral could be simplified into highly oscillatory line integrals in the following way:

$$I^{(a,b)} = \int_{L_1}^{L_2} \int_{ax+b}^{0} p(x',y') e^{ik(-x'^2+y'^2)} dy' dx'$$

=
$$\int_{L_1}^{L_2} \left(J_2^{(0,0)}(x') - J_2^{(a,b)}(x') \right) e^{-ikx'^2} dx'.$$
(6)

Here, the coordinate system for (x, y) is defined with respect to the use of the polygonal boundary.

 $J_2^{(0,0)}(x)$ and $J_2^{(a,b)}(x)$ have the formulations

$$J_2^{(0,0)}(x) = j_1(x) + j_2^{(0,0)}(x)$$

$$J_2^{(a,b)}(x) = j_1(x) \operatorname{erfc}\left(\sqrt{-ik(ax+b)}\right) + j_2^{(a,b)}(x) e^{ik(ax+b)^2}.$$

where

$$j_1(x) = -\frac{\sqrt{\pi}}{2\sqrt{-ik}} \left(\alpha_1 + \alpha_2 x + \alpha_4 x^2 - \frac{\alpha_5}{2ik}\right)$$
$$j_2^{(a,b)}(x) = \frac{\alpha_3 + \alpha_6 x + \alpha_5(ax+b)}{2ik}, j_2^{(0,0)}(x) = \frac{\alpha_3 + \alpha_6 x}{2ik}.$$

Hence, the original PO integral $I^{(a,b)}$ in (6) can be rewritten as

$$I^{(a,b)} = I_2^{(0,0)} - I_2^{(a,b)}$$
(7)

where

$$I_{2}^{(a,b)} = \int_{L_{1}}^{L_{2}} J_{2}^{(a,b)}(x') e^{-ikx'^{2}} dx'$$

$$I_{2}^{(0,0)} = \int_{L_{1}}^{L_{2}} J_{2}^{(0,0)}(x') e^{-ikx'^{2}} dx'.$$
(8)

Here, $I_2^{(a,b)}$ and $I_2^{(0,0)}$ are line integrals associated with edges $\mathbf{V}_1\mathbf{V}_2$ and $\mathbf{V}_3\mathbf{V}_4$, respectively. $J_2^{(a,b)}(x)$ has complicated formulations involving the complementary error functions. Importantly, the difference between this communication and the paper in [19] is that the phase term e^{-ikx^2} was adopted in this work, while e^{ikx^2} was considered in [19]. This difference is due to the consideration of the hyperbolic surface in this communication.

The integrand $J_2^{(a,b)}(x)$ in (8) has the following asymptotic behavior:

$$J_2^{(a,b)}(x) = \begin{cases} \varsigma_1(x)e^{ik(ax+b)^2}, & x \in \mathcal{D}_1\\ 2j_1(x) + \varsigma_2(x)e^{ik(ax+b)^2}, & x \in \mathcal{D}_2 \end{cases}$$
(9)

with $\varsigma_1(x)$ and $\varsigma_2(x)$ denoted as slowly varying functions.

 \mathcal{D}_1 and \mathcal{D}_2 are the domains separated by the Stokes' line on the complex plane, with the expressions

$$l_{\text{Stokes}}(x) : \text{Im}(x) = -\text{Re}(x) - \frac{b}{a}$$
(10)

$$\mathcal{D}_1 := a \left(\operatorname{Re}(x) + \operatorname{Im}(x) \right) + b > 0 \tag{11}$$

$$\mathcal{D}_2 := a \left(\operatorname{Re}(x) + \operatorname{Im}(x) \right) + b < 0.$$
(12)

For the case $x \in D_2$ in (9), the first term $2j_1(x)$ comes from the Stokes' phenomenon of the complementary error function as shown in Fig. 4, details could be found in [19]. After substituting (9) into (8), we get two phase function terms for $I_2^{(a,b)}$. They are

$$g_1(x) = -x^2 + (ax+b)^2, \quad g_2(x) = -x^2.$$
 (13)



Fig. 4. Stokes' phenomenons of the complementary error functions, erfc $(\sqrt{-ik}(0.5x+1)) - 2$ and erfc $(\sqrt{-ik}(0.5x+1))$.

The Stokes' phenomenon of complementary error function makes the phase behaviors of the PO integrand $I_2^{(a,b)}$ be discontinuous.

Now we consider the phase function $g_1(x)$ of $I_2^{(a,b)}$ in (13). Physically, there may exist a point x_s , at which the phase behavior of $g_1(x)$ is different from others. It is called the stationary phase point (SPP). SPP corresponds to the point at which the specular reflection occurs in the high frequency ray physics regime. Mathematically, the SPP x_s satisfies the condition $g'_1(x_s) = 0$. As a result, we have the expression of x_s as

$$x_{s} = \begin{cases} \frac{ab}{1-a^{2}}, & |a| \neq 1\\ \text{no SPP,} & |a| = 1. \end{cases}$$
(14)

Remark 1: For the case |a| = 1 in the above formulation, the phase function in (13) reduces to a linear form $g_1(x) = 2abx + b^2$. Hence, there is no SPP.

Now, we see the term $e^{ikg_1(x)}$ in the PO integrand

$$e^{ikg_1(x)} = e^{ik\left[\operatorname{Re}(g_1(x)) + i\operatorname{Im}(g_1(x))\right]} = e^{-k\operatorname{Im}(g_1(x)) + ik\operatorname{Re}(g_1(x))}.$$
 (15)

Here, $g_1(x)$ is a real function. In this work, we adopt the NSDP method. We consider the real and imaginary parts for the consideration of the NSDP on the complex plane. The NSDP method relies on the transformation of the above highly oscillatory functions to exponential decay functions on the complex plane. In detail, for a starting point L_* , we define a complex path function $x = \varphi_{L_*}(p)$ as that in [2], satisfying the following identity:

$$-\varphi_{L_*}(p)^2 + (a\varphi_{L_*}(p) + b)^2 = -L_*^2 + (aL_* + b)^2 + ip^l \quad (16)$$

with l = 1 for integration end points L_1 and L_2 , and l = 2 for the SPP x_s , respectively. Here, p is the path parameter for the path function on the complex plane. In (16), L_* could be used to represent the integration end points L_1 and L_2 , as demonstrated in Fig. 4.

After substituting L_1 , L_2 , and x_s into (16), the corresponding NSDPs are

$$\varphi_{L_m}(p) = \begin{cases} \frac{\operatorname{sgn}(L'_m)}{\sqrt{a^2 - 1}} \sqrt{{L'_m}^2 + ip} + x_s, & \text{if} |a| > 1\\ \frac{\operatorname{sgn}(L'_m)}{\sqrt{1 - a^2}} \sqrt{{L'_m}^2 - ip} + x_s, & \text{if} |a| < 1 & (17)\\ L_m + \frac{ip}{2ab} & \text{if} |a| = 1 \end{cases}$$
$$\varphi_{x_s}(p) = \begin{cases} \frac{\sqrt{ip}}{\sqrt{|1 - a^2|}} + x_s, & if|a| > 1\\ \frac{\sqrt{-ip}}{\sqrt{|1 - a^2|}} + x_s, & \text{if} |a| < 1 & (18)\\ \text{no NSDP}, & \text{if} |a| = 1 \end{cases}$$



Fig. 5. (a) PO surface integral I_{Δ_1} defined on the triangular patch, Δ_1 . (b) NSDPs diagram for $I_2^{(a_1,b_1)}$ defined on the edge $\mathbf{V}_1\mathbf{V}_2$ of Δ_1 . (c) NSDPs diagram for $I_2^{(a_2,b_2)}$ defined on the edge $\mathbf{V}_2\mathbf{V}_3$ of Δ_1 . (d) NSDPs diagram for $I_2^{(a_3,b_3)}$ defined on the edge $\mathbf{V}_1\mathbf{V}_3$ of Δ_1 .

with $p\in [0,\infty)$ and $p\in (-\infty,\infty)$ in (17) and (18), respectively. Here,

$$L'_{m} = \sqrt{|1-a^{2}|} \left(L_{m} - \frac{ab}{1-a^{2}} \right) = \sqrt{|1-a^{2}|} (L_{m} - x_{s})$$

m = 1, 2. For instance, the diagrams of NSDPs in (17) and (18) with |a| = 1, |a| > 1, and |a| < 1, are demonstrated in Fig. 5(b)–(d), which correspond to three NSDPs defined on three edges of the triangular patch.

IV. PO FORMULATIONS ON TRIANGULAR PATCHES BY THE NSDP METHOD

After finding the NSDPs in Section III, we give the result of PO surface integral formulations in (4) on triangular patches. First, the surface PO integral defined on Δ_1 in Fig. 5(a) can be separated into three line integrals

$$I_{\Delta_1} = I_2^{(a_1,b_1)} + I_2^{(a_2,b_2)} - I_2^{(a_3,b_3)}.$$
 (19)

Then, on invoking the Cauchy's integral formulation and following the similar mathematical manipulations as those in [19], the above three highly oscillatory line integrals can be rewritten as

$$I_{2}^{(a_{1},b_{1})} = I_{2,\mathbf{V}_{1,x}}^{(a_{1},b_{1})} - I_{2,\mathbf{V}_{2,x}}^{(a_{1},b_{1})}$$
(20)

$$I_{2}^{(a_{2},b_{2})} = I_{2,\mathbf{V}_{2,x}}^{(a_{2},b_{2})} + I_{2,\mathbf{X}_{r,2,x}}^{(a_{2},b_{2})} - I_{2,\mathbf{V}_{3,x}}^{(a_{2},b_{2})}$$

$$+ K_2 \left((\mathbf{V}_{3,x}, 0) \right) - K_2 \left(\mathbf{A}^{(2)} \right)$$
(21)

$$I_{2}^{(a_{3},b_{3})} = I_{2,\mathbf{V}_{1,x}}^{(a_{3},b_{3})} + I_{2,\mathbf{X}_{r,3,x}}^{(a_{3},b_{3})} - I_{2,\mathbf{V}_{3,x}}^{(a_{3},b_{3})} + K_{2}\left(\left(\mathbf{V}_{3,x},0\right)\right) - K_{2}\left(\mathbf{C}^{(3)}\right).$$
(22)

Here, in (20)–(22), $\mathbf{V}_n = (\mathbf{V}_{n,x}, \mathbf{V}_{n,y})$ denotes the vertex points of $\Delta_1, n = 1, 2, 3$. The variables $\mathbf{V}_{n,x}, \mathbf{V}_{n,y}$ represent the x- and y- values of the vertex points \mathbf{V}_n . $\mathbf{A}^{(2)}$ and $\mathbf{C}^{(3)}$ denote the intersection

points between the NSDPs and the Stokes' line [19]. The superscripts "2" and "3" represent the second and third edges of the triangular patch, as shown in Fig. 4. The resonance points $\mathbf{X}_{r,m}$ in Fig. 5(a) are denoted as

$$\mathbf{X}_{r,m} = (\mathbf{X}_{r,m,x}, \mathbf{X}_{r,m,y}) = \left(\frac{a_m b_m}{1 - a_m^2}, \frac{b_m}{1 - a_m^2}\right)$$
(23)

 a_m and b_m correspond to the variables from three edges of Δ_1 , with the formulations $y_m(x) = a_m x + b_m$, m = 2, 3. The above $I_{2, \mathbf{V}_{m,x}}^{(a_n, b_n)}$ and $I_{2, \mathbf{X}_{r,m,x}}^{(a_n, b_n)}$ in (20)–(22) are similar as (30) and (31) given in [19] except the different NSDPs in (17) are adopted. $K_2(x)$ takes the formulation

$$K_{2}(x) = \left(\frac{\pi}{2k}\alpha_{1} + \frac{\pi}{4ik^{2}}\alpha_{4} - \frac{\pi}{4ik^{2}}\alpha_{5}\right)\operatorname{erfc}\left(\sqrt{ikx}\right) + \left(\frac{\sqrt{\pi}}{2ik\sqrt{-ik}}\alpha_{2} + \frac{\sqrt{\pi}x}{2ik\sqrt{-ik}}\alpha_{4}\right)e^{-ikx^{2}}.$$
 (24)

Remark 2: ****The PO surface integral can always be reduced to highly oscillatory integrals defined on polygonal edges. In other words, for assembled triangular patches, internal vertex and resonance points' contributions are canceled with each other [18].

A. Analysis of Critical-Point Contributions by the NSDP Method

When the working frequency is high, the PO-based EM fields in (1) can be separated into high-frequency critical-point contributions [2], [7]. In Fig. 5(a), these critical points consist of the SPP X_s (SPP), the boundary resonance points $X_{r,m}$ (RSPs) and the vertex points V_n (Vexs), m = 2, 3, n = 1, 2, 3.

Similarly to the discussions in [20], on invoking the NSDP method, the critical-point contributions for the PO integral in (19) take the forms

$$I_{\Delta_1}^{(\text{NSDP, SPP)}} = \underbrace{K_2\left(\mathbf{C}^{(3)}\right) - K_2\left(\mathbf{A}^{(2)}\right)}_{(25)}$$

$$I_{\Delta_1}^{(\text{NSDP, RSPs})} = I_{2,\mathbf{x}_{r,2,x}}^{(a_2,b_2)} - I_{2,\mathbf{x}_{r,3,x}}^{(a_3,b_3)}$$
(26)

$$I_{\Delta_{1}}^{(\text{NSDP, Vexs})} = \underbrace{I_{2,\mathbf{V}_{1,x}}^{(a_{1},b_{1})} - I_{2,\mathbf{V}_{1,x}}^{(a_{3},b_{3})} + I_{2,\mathbf{V}_{2,x}}^{(a_{2},b_{2})} - I_{2,\mathbf{V}_{2,x}}^{(a_{1},b_{1})}}_{+ \underbrace{I_{2,\mathbf{V}_{3,x}}^{(a_{3},b_{3})} - I_{2,\mathbf{V}_{3,x}}^{(a_{2},b_{2})}}_{\text{contributions from three vertex points}}.$$
(27)

Here, $I_{\triangle_1}^{(\text{NSDP, SPP})}$, $I_{\triangle_1}^{(\text{NSDP, RSPs})}$, and $I_{\triangle_1}^{(\text{NSDP, Vexs})}$ denote the contributions coming from \mathbf{X}_s , $\mathbf{X}_{r,m}$, and \mathbf{V}_n , respectively. As a result, comparing (25)–(27) with I_{\triangle_1} in (19), we arrive at

$$I_{\triangle_1} = I_{\triangle_1}^{(\text{NSDP, SPP})} + I_{\triangle_1}^{(\text{NSDP, RSPs})} + I_{\triangle_1}^{(\text{NSDP, Vexs})}.$$
 (28)

The above critical-point contributions via the HFA method are presented in [9], [14], and [20]. Furthermore, by the HFA theory, the asymptotic behaviors of contributions coming from SPP, RSPs, and vertices are of orders $O(k^{-1})$, $O(k^{-1.5})$ and $O(k^{-2})$, respectively. In other words, the specular reflection contribution by the SPP is the dominant term in the PO-based EM fields [9], [14]. Furthermore, we shall note the similarity and difference of the uniform asymptotic solutions in [9] and [14]. By performing uniform asymptotic techniques in [9] and [14] for high-frequency critical points, nonuniform leading terms have the similar formulations. However, when the observation points lie around shadow boundaries, formulations are different in [9] and [14]. Thus, different accuracies in [9] and [14] will be generated from asymptotic solutions.



Fig. 6. (a) PO surface integral I_{\triangle} defined on the triangular patches, which are moving along the line l(x) = 0.5x denoted by the red color row. (b) Amplitude of the PO surface integrals from the triangular patches that are moving along the line l(x) = 0.5x, $x \in [-3, 5]$.

V. NUMERICAL RESULTS

We first consider the coalescence of the critical points on the triangular patch with the hyperbolic phase behavior, which are shown in Fig. 6(a). The triangular patches are moving along a line l(x) = 0.5x, $x \in [-3, 5]$. In particular, with x = -2, the edge $\mathbf{V}_2\mathbf{V}_3$ is governed by the line y = -2x. Then, the SPP \mathbf{X}_s and the resonance point $\mathbf{X}_{r,3}$ come together. As shown in Fig. 6(b), the contributions by the NSDP and brute force methods agree well with each other, even when \mathbf{X}_s and $\mathbf{X}_{r,3}$ come together. To compare the results among the NSDP, the HFA and the BF methods, we consider the case x = 0. Then, the SPP lies inside of the triangular patch. The PO integral results are $I_{\Delta} = 0.0291, 0.0290, 0.0278$ by the NSDP, BF, and HFA methods, respectively.

We consider the hyperbolic surface in Fig. 2(a). The governing equation of the hyperbolic surface is f(x, y) = 1 - 0.06 $(-x^2 + xy + y^2)$. The resultant PO-based EM fields is expressed in (1). $\partial \Omega_{xy}$ is the quadrilateral domain $\mathbf{V_1V_2V_3V_4}$ shown in Fig. 2(b), with the vertex points $\mathbf{V_1} = (-5.6036, 0.7987)$, $\mathbf{V_2} = (2.3455, 5.7115)$, $\mathbf{V_3} = (2.9254, -4.1142)$, and $\mathbf{V_4} = (8.9043, 5.0974)$. The incident wave propagates along $\hat{\mathbf{r}}^{(i)} = [0.5, 0.5, -\sqrt{2}/2]$ direction, and the observation point is set along the direction $\hat{\mathbf{r}} = [\sqrt{2}/4, \sqrt{6}/4, \sqrt{2}/2]$.

By applying the NSDP method, we could generate the PO-based EM fields results. Meanwhile, another way to generate PO-based EM fields results is the HFA method [7], [9]. In this communication, we consider the case that the critical points are isolated. Hence, we adopt the nonuniform solutions for the PO-based EM fields. Meanwhile, we note that critical-point transitional behaviors are neglected in the asymptotic analysis, which leads to low-accuracy results generated for the PO-based EM fields. If the uniform asymptotic technique with the



Fig. 7. Comparisons of the RCS (dBsm unit) values of the PO-based EM fields on the hyperbolic surface by using the NSDP and BF methods.



Fig. 8. Comparisons of the CPU time (second unit) for the PO-based EM fields by using the NSDP and BF methods.

TABLE I Comparisons of the Errors of $\mathbf{E}^{(s)}(\mathbf{r})$ Results by Using the NSDP and HFA Methods Relative to the BF Method

k (1/m)	HFA-error	NSDP-error	NSDP-CPU	BF–CPU
10	4.613342E-3	5.719708E-9	10.1089	4.9296
50	6.244134E-4	1.450380E-13	8.9077	24.0866
100	1.225014E-4	7.211293E-12	8.8609	48.2979
200	7.728819E-5	4.616638E-8	8.9857	96.1590
300	3.698174E-5	1.144945E-5	8.6581	169.0427
500	1.945051E-5	4.181301E-5	8.9701	242.8624

UTD transition function is adopted, one could estimate high accuracy as the consideration of transitional contributions for critical points. We will consider the uniform-asymptotic technique in the future.

In Fig. 7, we apply the NSDP method to calculate the bistatic RCS values of $\mathbf{E}^{(s)}(\mathbf{r})$, which are in good agreement with the results generated by the BF method. Fig. 8 demonstrates the frequency-independent computational effort for the scattered electric field. Finally, Table I gives comparisons of the errors of $\mathbf{E}^{(s)}(\mathbf{r})$ produced by NSDP and HFA methods relative to the BF method. Compared with the HFA method, the advantage on improving the scattered electric field accuracy by the NSDP method is again confirmed in Table I. In summary, on invoking the proposed NSDP method, the PO-based EM fields on the quadratic hyperbolic surface could be calculated with frequency-independent workload and error controllable accuracy.

VI. CONCLUSION

In this communication, we propose the NSDP method to calculate the PO-based EM fields on the quadratic hyperbolic surface. The scattered electric field can be reduced to several highly oscillatory PO surface integrals. By deforming the original PO integration path to the NSDP on the complex plane, each PO integrand decays exponentially. Extensive numerical experiments are given to show the efficiency of the NSDP method. In conclusion, the NSDP method for calculating the electric scattered field on the quadratic hyperbolic surface is frequency independent and error controllable.

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A Novel Simple and Compact Microstrip-Fed Circularly Polarized Wide Slot Antenna With Wide Axial Ratio Bandwidth for C-Band Applications

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Abstract—This communication presents a design of a new compact circularly polarized (CP) slot antenna fed by a microstrip feedline. The 3-dB axial ratio band can be achieved by simply protruding a horizontal stub from the ground plane toward the center of the wide slot (WS) and then feeding the WS with a microstrip feedline positioned to the side of the WS, underneath the protruded stub. The feedline and metallic stub are perpendicular to each other, and they resemble a T shape when viewed from the top. The proposed antenna is fabricated with an area of $25 \times 25 \text{ mm}^2$. Measurement results show that the antenna attains an $S_{11} \leq -10 \text{ dB}$ impedance matching bandwidth of 90.2%, from 3.5 to 9.25 GHz, and a broadband 3 dB-AR bandwidth of 40%, ranging from 4.6 to 6.9 GHz. A peak gain of 0.8–4.5 dBi is achieved within the AR band. The proposed antenna is suitable for circular polarization applications in C band.

Index Terms-Axial ratio, circularly polarized (CP), slot antenna.

I. INTRODUCTION

Recently, due to the increasing demands for communication systems, the research on small antennas with various radiating elements, feeding structures, and polarizations have attracted enormous attentions. Due to its advantages of better mobility and weather penetration compared with linearly polarized (LP) antennas, the circularly polarized (CP) antenna is getting popular in wireless communication systems. In recent years, lots of researches have gone into designing CP WS antennas because of the advantages of wide bandwidth, low

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TABLE I CP Bands and Sizes of Some Existing Ring- and Wide-Slot Antennas

Ref.	Ant.	f_c	3-dB	Ant. area
	type	(MHz)	ARBW	$(mm \times mm), (\lambda_0^2)$
			(%)	pr Andre in Draght
(1)	WS	2413	28.8	60 × 60, 0.233
(2)	WS	5790	32.2	60 × 60, 1.341
(3)	WS	3575	85.0	60 × 60, 0.511
(4)	WS	2500	16.0	$30 \times 46, 0.096$
(5)	WS	2220	30.6	60 × 60, 0.197
(6)	WS	1575	3.81	$60 \times 60, 0.099$
(7)	RS	3030	57.4	106.5 × 106.5, 1.157
(8)	RS	3700	27	50 × 50, 0.381
(9)	RS	2165	32.8	$60 \times 60, 0.187$
(10)	RS	3000	46.7	65 × 35, 0.228
(11)	Array	1550	52	$220 \times 220, 1.292$
(12)	Array	1445	120	$180 \times 180, 0.752$
Proposed	WS	5750	40	$25 \times 25, 0.230$

profile, and easy integration with monolithic microwave-integrated circuits. The operating principle of CP antennas is to excite two orthogonal modes with equal amplitude and in-phase quadrature. This can be achieved by introducing some symmetric and/or asymmetric perturbations into the wide-slot (WS) or ring-slot (RS) antenna [1]–[12]. These include embedding two L-ground strips on opposite corners of a square-slot antenna [1], [2], and adding a third L-grounded strip in the square slot to enhance the AR bandwidth [3]. Also utilizing perturbations in the forms of: feed lines [4]–[6], slot structures [7]–[10], and array configurations [11], [12] have also been proposed. However, antenna configurations of these designs are so complicated that they lead to complexity in antenna designs and fabrications.

In this communication, a new, yet structurally simple, and compact broadband CP antenna is proposed. The presented antenna consists of a rectangular slot, a microstrip feedline, and a horizontal stub protruded from the ground plane. A broadband CP operation can be achieved by simply positioning the microstrip feedline beneath the extended stub. The proposed antenna possesses a large AR bandwidth with its simple configuration and compact structure. In this design, the 3-dB AR bandwidth reaches as large as 2.3 GHz which is about 40% (relative to its center frequency of 5.75 GHz) to cover the WLAN (5.2, 5.8 GHz), WiMAX (5.5 GHz), and other wireless systems in C band. Table I shows the performances of the proposed antenna and antennas in references [1]–[12].

II. ANTENNA DESIGN

The geometry of the proposed CP slot antenna is illustrated in Fig. 1. As shown in Fig. 1, the proposed antenna is fed by a $50-\Omega$ microstrip feedline printed on top of the FR4 substrate (relative permittivity $\varepsilon_r = 4.4$, height = 1.6 mm). The width of the feedline is 3 mm. The ground plane is printed on the bottom of the substrate. A large slot is introduced in the ground plane of the antenna. A stub is then protruded from the right side of the ground plane toward the center of the slot. A gap is created on the ground plane above the feedline to reduce coupling between the feedline and the ground plane. The overall size is $25 \times 25 \text{ mm}^2$, and the antenna is printed on the *xoy* plane. To realize broadband CP operation, the microstrip feedline is placed on the right edge of the antenna beneath the protruded stub.

The evolution of the proposed antenna is depicted in Fig. 2 to explain the CP performance of the antenna. Four antennas have been

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